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Magnetic Antennas and Magnetic Probes

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Abstract – In the paper are presented designs and applications of magnetic field radiators and sensors mainly in the aspect of basic bioelectromagnetic studies and measurements related to H-field measurements for labor safety and environment protection purposes.

Keywords – H-field sources; exposure systems and measurement; bioelectromagnetics; labor safety; environment protection; electromagnetic compatibility.

I. INTRODUCTION

The magnetic field generation and sensing is mainly based upon loop antennas applications. Although the size of a loop (in electrical sense) may be arbitrary one, presented deliberations are focused upon small-size devices. The approach is a result of the authors' involvement in the area of the standard ElectroMagnetic Field (EMF) generation and metrology for susceptibility studies. Especially in bioelectromagnetics and generally understood EM environment protection. It requires a special attention to be paid to phenomena characterizing the near-field that usually are omitted in considerations related to telecommunications, limited to the far-field.

The paper is based mainly on the authors experience and their proposals related to new solutions and applications of H-field standards, exposure systems and the field sensing. Till now presented ideas [1, 2] are widened and the newest concepts are added.

II. A LOOP AS A TRANSMITTING ANTENNA

The main advantage of the loop antenna is a possibility to design a resonant loop even at very low frequencies. A concurrent solution, sometimes used in telecommunications, is here a whip antenna. Let's briefly compare the both solutions.

The input resistance of a short whip (ground plane antenna) R_w , over perfectly conducting ground, is expressed by [3]:

$$R_w = 10(kh)^2 \quad (1)$$

Where: h is a length of the whip,
 $k = 2\pi/\lambda$ – propagation constant,
 λ is the wavelength.

The losses resistance of the whip R_{wl} is given by [4]:

$$R_{wl} \approx \frac{100 \cdot 10^{-6} h}{r} \sqrt{\frac{f}{\sigma}} \quad (2)$$

Where r is the radius of the whip wire,
 f is frequency,
 σ is conductivity of the wire.

Combining both the formulas we may evaluate the radiation efficiency of the whip η_w :

$$\eta_w \approx \frac{1}{1 + R_{wl} / R_w} \quad (3)$$

Similar considerations for the small loop give its radiation resistance R_l [3] and the losses resistance R_{ll} [4] in the following form:

$$R_l = 320\pi^4 (nS\lambda^{-2})^2 \quad (4)$$

and:

$$R_{ll} = \frac{315 \cdot 10^{-6} nc}{r} \sqrt{\frac{f}{\sigma}} \quad (5)$$

Where S is the loop surface,
 n is number of turns,
 c is the loop circumference.

Both the formulas allow to introduce radiation efficiency of the loop η_l :

$$\eta_l = \frac{1}{1 + 0.82 \cdot 10^{26} c / rnS^2 \sigma^{1/2} f^{7/2}} \quad (6)$$

An important parameter of a transmitting antenna is its efficiency. Strict analysis of presented formulas allows to conclude that the loop antenna, as a transmitting one, is more effective at frequencies below several megahertz. The efficiency of the whip, as given by formula 3, was introduced for ideal ground. The real earth (or other type of counterpoise) reduces the efficiency and makes it dependent from the earth conductivity. An advancement of the loop is its relatively small sensitivity to surroundings and a possibility to increase a current feeding the loop in Q -times (where Q is quality factor of the loop) while the loop is tuned to resonance.

III. A LOOP AS A RADIATOR

As may be concluded from the above considerations a loop antenna, as a transmitting antenna, has several advancements at relatively low frequencies. In our case, as a radiator, has important possibility: a generation of H-field which parameters (intensity, polarization) may be precisely calculated. The first application here is a H-field standard.

The basic set of a H-field standard, widely applied for H-field meters calibration, is shown in Fig. 1.

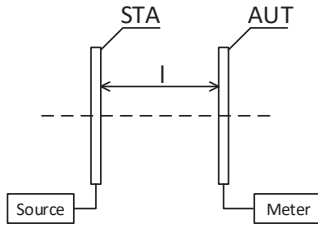


Fig. 1 H-field meter calibration

Axially, at distance l from a standard transmitting antenna (STA) is placed loop antenna of a calibrated meter (AUT). The average H-field intensity (H_{av}), at the surface of the antenna, in the first approximation, is given by [1]:

$$H_{av} = \frac{IS}{2\pi l^3} \sqrt{1+k^2 l^2} \quad (7)$$

Where I is current feed to the STA.

This approach is applied for H-field probes calibration in wide frequency range as well as for selective E-field meters designated for propagation studies at frequencies below 30 MHz. Apart from an loop antenna, in the latter case, the meters shows indications in E-field units. It is often forgotten that the procedure is valid only for the far-field conditions, where relation between the both field components is constant and equals $E = HZ_0$ (where Z_0 is intrinsic impedance of free space, $Z_0 = 120\pi$ ohms). The procedure is invalid in the near-field conditions.

Similar set as above may be used in so called substitution method. In this method a role of a radiator may be played by arbitrary loop. Thus, at distance l , coaxially to the radiating loop, is firstly placed a standard receiving antenna (SRA) and then it is replaced by an antenna of calibrated meter. One of our first improvements, which allow an increase the calibration procedure accuracy, was a proposal of the double calibration method. The idea of the calibration is shown in Fig. 2.

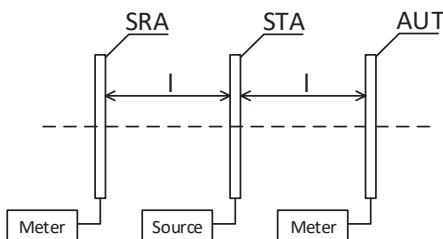


Fig. 2 Double calibration method

In the center, between a SRA and an antenna under test (AUT) is placed a STA. The set allows simultaneous calibration using both the methods. Then a replacement of SRA and AUT and distances l makes it possible to reduce calibration errors and a more accurate estimation of the calibration accuracy. The bench for H-field probes double calibration, in the authors' lab, is shown in Fig. 3.

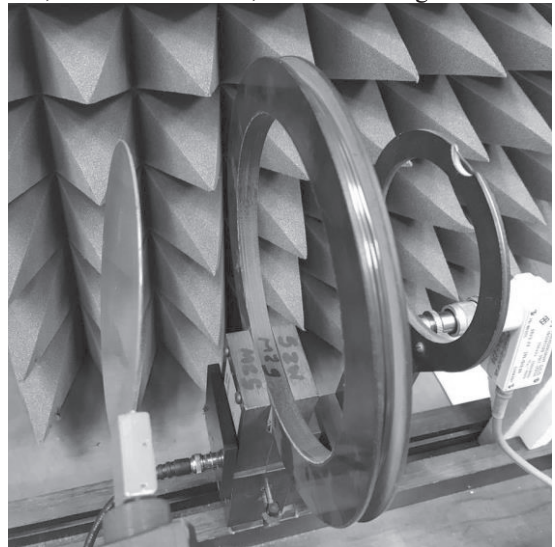


Fig. 3. Double calibration of a H-field probe

Another possibility of the set shown in Fig. 1 is its use for whip and dipole antennas calibration. Such a calibration especially performed at lower frequencies. The use of traditional methods using for calibration standard whips or dipoles, is sensitive to geometry of propagation between radiating and calibrated antenna, surroundings and even wiring configuration. It makes the approach troublesome and inaccurate. Proposed method assures more stable and accurate calibration and is more comfortable and easier in the use. An idea of the method is shown in Fig. 4.

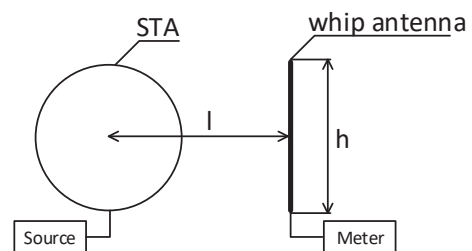


Fig. 4. A whip antenna calibration

A whip (or dipole) antenna of length h is placed at distance l from the STA, in the plane of the STA. Average E-field intensity E_{av} , at the calibrated antenna length is given, in the first approximation, by [1]:

$$E_{av} = \frac{IS}{2\pi l^3} \sqrt{1+k^2 l^2} \quad (8)$$

An input impedance of a loop antenna, well below its resonant frequency, is majorized by imaginary part of the impedance. The reactance is proportional to frequency. Thus, if the antenna is fed with a constant voltage, the H-field intensity increases proportionally with frequency. This effect may make more difficult measurements of a frequency response of wideband H-field probes. Although it is possible to take into account this effect in computer controlled calibration systems, in order to simplify the procedure was proposed to feed the STA through a low band-pass filter is set as shown in Fig. 5.



Fig.5. A frequency independent concept.

In above presented considerations and solutions a polarization of the field was not taken into account. For the far-field meters calibration in linear polarized H-field is enough. Traditional calibration of omnidirectional H-field probes, containing three mutually independent loops, was performed by triple calibration – separate for any of the probe's three loops. A bit more advanced method has been proposed. The method is almost identic to the solution presented in Fig. 1, however includes two identic STAs, placed perpendicular one to each other and fed with a current in the quadrature, as shown in Fig. 6.

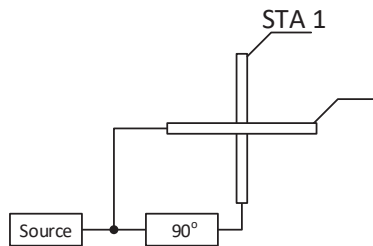


Fig. 6 H-field standard with circular polarization.

All the above designs may be applied both as primary standards for meters calibration (as discussed) and as exposure systems for electromagnetic compatibility (EMC) purposes. As far as susceptibility to H-field of nonliving devices or materials is performed the linear polarization may be enough; however, in the case of exposure *in vivo* the approach leads to errors in the real exposure estimations as absorbed energy of the field depends upon position of an exposed animal in relation to the field vector (-s). Thus, it is possible (and, unfortunately, widely applied in bioelectromagnetic experiments) to immobilize the animal; however, a stress due to the immobilization may totally falsify results of the experiment. In the case of animal's unlimited behavior a precise estimation of EMF energy deposited (absorbed) in the animal's body is impossible. The best solution it would be a spherical polarized field. Unfortunately, such a solution is physically impossible. Thus, a quasispherical polarization is proposed. An idea of the polarization is shown in Fig. 7.

Three, mutually perpendicular and placed coaxially, loops are fed with currents given by formulas:

$$\begin{aligned} I_1 &= A \cos(\Omega t + \Phi) \\ I_2 &= B \sin(\Omega t + \Phi) \sin(\omega t + \varphi) \\ I_3 &= C \sin(\Omega t + \Phi) \cos(\omega t + \varphi) \end{aligned} \quad (9)$$

Where: I_1 , I_2 and I_3 are currents fed to separate antennas,

Ω is a carrier wave frequency,

Φ is phase of the carrier wave,

ω is a rotating frequency,

φ is phase of the rotating frequency

A, B and C are amplitudes.

The vector sum of the currents (and, as a result, generated by them H-fields, for $A = B = C$, leads to a direction independent constant value – equal to the amplitude of generated H-field of quasispherical polarization. The field in the center of the loops is polarized circularly (elliptically) at the carrier wave frequency and then rotated in the space with auxiliary rotating frequency. It assures presence of three spatial components of the field. Selection of phases and amplitudes assure a possibility to generate H-field from linear to quasispherical polarization, arbitrary located and with arbitrary rotations' direction (left- and right-hand polarization).

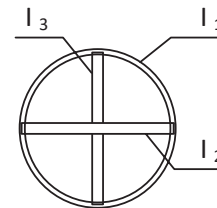


Fig. 7. A concept of quasispherical polarization.

Solution presented in Fig. 7 assures very limited volume in which uniformity of the field may be assumed as satisfying. In the case of larger objects exposure a set of three, mutually perpendicular Helmholtz coils is proposed as shown in Fig. 8.

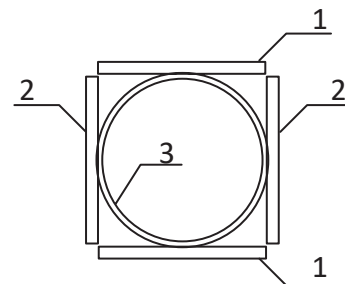


Fig. 8. Three Helmholtz coils.

Apart from quite uniform exposure of free moving animals presented solutions of quasispherical polarized fields may be of use in EMC studies as well. They would assure a possibility to study a response of an object under test to arbitrary polarized field without a necessity to move (turn) it.

IV. A LOOP AS A RECEIVING ANTENNA

Contrary to the transmitting case, here an effective high h_{eff} of the antenna is of concern. It is given by [2]:

$$h_{\text{eff}} = \frac{2\pi m S}{\lambda} \quad (10)$$

It means that the electromotive force, induced by the field in the loop, is frequency dependent. This is of secondary importance in loop antennas applied in the far-field E-field meters, H-field SRAs', ferrite rod antennas in radio-receivers and similar applications. However; it creates problems of twofold nature in the case of the loops playing a role of sensors in wideband, H-field meters:

1. The frequency response of wideband meter (probe) should be flat within the measuring frequency range. Required flatness is obtained by the way of the probe connection to it's' load via a low band-pas filter matched to the lower corner frequency of the probe (LF_1 , see Fig. 9).
2. Formula (10) is valid for small-size antennas. At higher frequencies an antenna may become resonant one and number of the resonants may be infinite one: the first at resonant frequency of the antennas' self-inductance and self-capacitance, including dispersed capacitances of the circuitry, the second at frequency at which the antenna reaches resonant sizes and farther at its any harmonic frequency. In order to eliminate deformations of the frequency response another low-pass filter (-s) (LF_2) is indispensable.

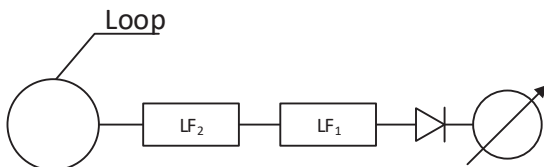


Fig. 9 Block diagram of a wide-band H-field meter

Another requirement to the near field meters, especially that designated for protection purposes, is an ability to simultaneous measure the three spatial H-field components. Solutions are known in the form of three probes (antennas) placed perpendicularly one to each other [5]. However; the solution, although widely used in meters offered at the market, is loaded by an inconvenience, that was never discussed or revealed before. As shown in Fig. 9 the output voltage of an antenna is detected by a diode. In an omnidirectional probe the output voltages of the three loops are summed. The pattern is omnidirectional if the sum is with square. Dynamic characteristic of a diode is square-law only in its beginning part, and then it becomes linear. Thus, as a result, the sum becomes linear as well. It results in the pattern deformations as deep as 3 dB, as shown in Fig. 10.

At the end it should be mentioned that H-field measurements for our purposes, especially at low frequencies, may be performed using other types of sensors; for instance: Hall cell, magneto-resistors or diodes and others. They were here omitted as the presentation is limited to antenna-type

sensors. The main advantages of the latter are their sensitivity and widebandness

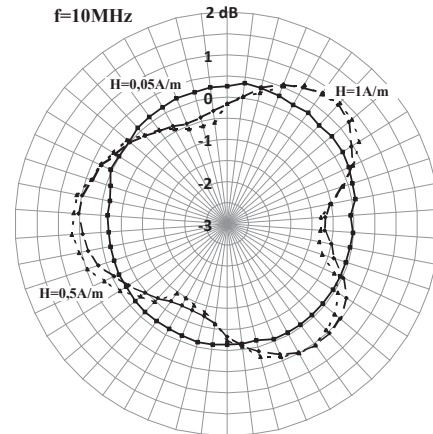


Fig. 10 Measured directional patten deformations of a omnidirectional H-field probe at two different field levels.

V. FINAL COMMENTS

In the paper several problems of H-field antennas were discussed. The main role in the considerations played a loop antenna in dual role: as a receiving and as a transmitting antenna. The considerations were limited mainly to the authors' involvement in the field of EMF standard fields generation (for H-field meters calibration an in a role of exposure systems) and H-field measurements, related to protection against unwanted exposure to EMF. All these problems are related to specific conditions of the near-field, where any approximations, specific to the far-field relationships, are nonacceptable.

The main aim of the authors work is a possibility to make discussed procedures easier, simpler and more accurate. The latter is the most important as the EMF measurements and standards are one of the least accurate within metrology of other physical magnitudes. The importance is justified by urgent necessity to precise estimation of a role played by electromagnetic environment pollution in humans and, especially in the conditions while more and more people is exposed to EMF and trends here are unidirectional.

In order to illustrate possibilities in the area several original solutions, proposed by the authors, are presented.

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