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H. Sira-Ramírez a, A. Luviano-Juárez a,b & J. Cortés-Romero a,c

a CINVESTAV-IPN Av. IPN No. 2508, Departamento de Ingeniería Eléctrica, Sección de Mecatrónica
b UPIITA-IPN Av. IPN No. 2580, Colonia Barrio la Laguna Ticomán, CP. 07340, México, D.F
c Facultad de Ingeniería, Departamento de Ingeniería Eléctrica y Electrónica, Universidad Nacional de Colombia, Carrera 30 No. 45-03 Bogotá, Colombia

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Flatness-based linear output feedback control for disturbance rejection and tracking tasks on a Chua’s circuit

H. Sira-Ramirez*, A. Luviano-Juárezab and J. Cortés-Romeroac

aCINVESTAV-IPN Av. IPN No. 2508, Departamento de Ingenierı́a Eléctrica, Seccı́on de Mecatrónı́ca; bUPIITA-IPN Av. IPN No. 2580, Colonia Barrio la Laguna Ticoman, CP. 07340, México, D.F; cFacultad de Ingenierı́a, Departamento de Ingenierı́a Eléctrica y Electrónica, Universidad Nacional de Colombia, Carrera 30 No. 45-03 Bogotá, Colombia

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A linear output feedback controller is developed for trajectory tracking problems defined on a modified version of Chua’s circuit. The circuit modification considers the introduction of a flat input, i.e. a suitable external control input channel guided by (a) the induction of the flatness property on a measurable output signal of the circuit and (b) the physical viability of the control input. A linear active disturbance rejection control based on a high-gain linear disturbance observer, is implemented on a laboratory prototype. We show that the state-dependent disturbance can be approximately, but arbitrarily closely, estimated through a linear high-gain observer, called a generalised proportional integral (GPI) observer, which contains a linear combination of a sufficient number of extra iterated integrals of the output estimation error. Experimental results are presented in the output reference trajectory tracking of a signal generated by an unrelated chaotic system of the Lorenz type. Laboratory experiments illustrate the proposed linear methodology for effectively controlling chaos.

Keywords: Chua’s circuit; linear control of chaotic systems; observers

1. Introduction

The problem of controlling chaotic systems has been approached from many perspectives. Efforts have been presented outside the realm of feedback control (feedforward or open-loop schemes). In the seminal paper by Ott, Grebogi, and Yorke (1990), the control problem is solved using results from perturbation theory. Those methodologies, however, exhibit a lack of robustness. Regarding feedback control methods, considerable attention has been devoted to nonlinear feedback control strategies. Passivity-based control has been proposed where chaotic dynamical system stabilisation can be analysed in terms of energy properties (Fradkov and Markov 1997; Pogromsky 1998; Qi, Zhao, and Song 2004). Other techniques include: active control (Njah and Vincent 2008), adaptive control (Tang 2008), backstepping design (Peng and Chen 2008), flatness-based control (Marquez and Sira-Ramirez 1995) and sliding mode control (Yan, Hung, and Liao 2006) among others.

The induction of the differential flatness property on Chua’s circuit, via the prescription of an appropriate flat input channel (Waldherr and Zeitz 2008), allows for the trivialisation of the controller design task reducing the feedback control problem to that of a linear controllable time-invariant system. The original introduction of the flatness concept is due to (Fliess, Lévine, Martin, and Rouchon 1995). The reader is also referred to the books by Sira-Ramirez and Agrawal (2004) and Lévine (2009) for background on flatness. For an approximate, yet effective, disturbance observer design, the input-to-flat output relation can be simplified to a linear perturbed equation or to a fixed order ultra-local model, as defined in Fliess and Join (2009). The perturbation input lumps both external disturbance inputs and state-dependent nonlinear terms, into a single uniformly absolutely bounded disturbance function. This viewpoint transforms the original control task into one the of robustly controlling, via a linear output feedback controller, an externally perturbed chain of integrators (see Sira-Ramirez, Ramirez-Neria, and Rodriguez-Angeles (2010) and Sira-Ramirez, Velasco-Villa, and Rodriguez-Angeles (2009a) for robotic applications and Sira-Ramirez, Núñez, and Visairo (2009b) for a typical power electronics problem). The additive disturbance input can be effectively, though approximately, estimated via a linear high gain, observer. This information is used in approximately cancelling (at the controller stage) its effects on the trajectory tracking quality. The effects of the unknown disturbance input on the output reconstruction error dynamics (at the
observer stage) may be attenuated via a suitable linear combination of iterated integral injections of the output estimation error. This is precisely the dual procedure to that characterising disturbance input attenuation in generalised proportional integral (GPI) Control (Fließ, Marquez, Delaleau, and Sira-Ramírez 2002) and, hence, the observers we advocate may be properly called GPI observers. Both in GPI control and GPI observer design, the need for appropriate linear combinations of iterated integral errors is completely equivalent to the hypothesis of a self-updating internal model of the perturbation input as a time polynomial approximation.

GPI observer-based output feedback control of nonlinear uncertain systems is very much related to methodologies known as: Disturbance Accommodation Control (DAC) and Active Disturbance Rejection Control (ADRC). These approaches deal with the problem of cancelling, from the controller’s actions, endogenous and exogenous unknown additive disturbance inputs affecting the system. Perturbation effects are made available via suitable linear, or nonlinear, estimation efforts. The reader is invited to read the works of Johnson (1971, 2008), those of Han (2009) and the contributions made by Gao, Huang, and Han (2001), Gao (2006), Sun and Gao (2005) and Sun (2007). GPI observers are also intimately related to a radically new viewpoint in nonlinear state estimation, based on differential algebra, developed by Fließ, Join, and Sira-Ramírez (2008). GPI observers for chaotic system linear state reconstruction is presented in Luviano-Juárez, Cortés-Romero, and Sira-Ramírez (2010).

This article is organised as follows Section 2 presents an introduction to linear control of nonlinear differentially flat systems using a GPI observer-based control. The description of the controlled Chua’s circuit is given in Section 3 where the main problem is formulated. The experimental implementation of our proposed approach, in a laboratory prototype, and the corresponding trajectory tracking results are presented in Section 4. Finally, Section 5 presents some conclusions and suggestions for further work in this area.

2. Linear generalised proportional integral observer-based control of nonlinear flat systems

Consider the following problem: it is desired to estimate the phase variables of the scalar, n-th order, nonlinear system

$$y^{(n)} = \phi(t, y, \dot{y}, \ldots, y^{(n-1)})$$

(1)

for which it is assumed that a solution $$y(t)$$ exists, uniformly in $$t$$, for every given set of initial conditions: $$y_0, \dot{y}_0, \ldots, y^{(n-1)}_0$$, specified at time $$t=0$$. Assume, however, that the function $$\phi()$$ is completely unknown. Any solution $$y(t)$$ of the above differential equation trivially satisfies: $$y^{(n)}(t) = \phi(t, y(t), \dot{y}(t), \ldots, y^{(n-1)}(t))$$. We assume based on this fact that, as a time function, the n-th derivative of the solution $$y(t)$$, given by $$y^{(n)}(t)$$, admits m further time derivatives which are all uniformly absolutely bounded. In other words, there exists a constant $$K$$ such that,

$$\sup_{t} |\phi^{(m)}(t, y(t), \dot{y}(t), \ldots, y^{(n-1)}(t))| \leq K$$

(2)

Setting $$y_1 = y$$, $$y_2 = \dot{y}$$, \ldots, $$y_n = y^{(n-1)}$$, a state space model for such an uncertain system is given by

$$\dot{y}_j = y_{j+1}, \quad j = 1, \ldots, n-1$$

$$\dot{y}_n = \phi(t, y_1, y_2, \ldots, y_n)$$

(3)

We propose the following observer for the phase variables $$\{y_1, y_2, \ldots, y_n\}$$ associated with $$y$$, characterised by the states $$\hat{y}_1, \ldots, \hat{y}_n$$ and complemented by m output estimation error iterated integral injections, characterised by the variable $$z_1$$. We have

$$\dot{\hat{y}}_j = \hat{y}_{j+1} + \lambda_{n+m-j} (y_1 - \hat{y}_1), \quad j = 1, \ldots, n-1$$

$$\dot{\hat{y}}_n = z_1 + \lambda_m (y_1 - \hat{y}_1)$$

$$\dot{\hat{z}}_i = z_{i+1} + \lambda_{m-i} (y_1 - \hat{y}_1), \quad i = 1, \ldots, m-1$$

$$\dot{\hat{z}}_m = \lambda_0 (y_1 - \hat{y}_1)$$

(4)

Let the estimation error $$e_y$$ be defined as $$e_y = e_1 = y_1 - \hat{y}_1 = y - \hat{y}_1$$ with $$e_2 = y_2 - \hat{y}_2$$, etc.,

$$\dot{e}_j = e_{j+1} - \lambda_{n+m-j} e_1, \quad j = 1, \ldots, n-1$$

$$\dot{e}_n = \phi(t, y_1(t), y_2(t), \ldots, y_n(t)) - z_1 - \lambda_m e_1$$

$$\dot{z}_i = z_{i+1} + \lambda_{m-i} e_1, \quad i = 1, \ldots, m-1$$

$$\dot{z}_m = \lambda_0 e_1$$

(5)

It is not difficult to see that the estimation error $$e_y = e_1$$ satisfies, after elimination of all variables $$z_i$$, the following $$n+m$$th order perturbed linear differential equation,

$$\dot{e}^{(n+m)} + \lambda_{n+m-1} e^{(n+m-1)} + \ldots + \lambda_1 e_1 + \lambda_0 e_y = \phi^{(m)}(t, y_1(t), y_2(t), \ldots, y_n(t))$$

(6)

Clearly, if $$\phi^{(m)}()$$ is uniformly absolutely bounded, then choosing the gain coefficients, $$\lambda_j$$, $$j = 0, 1, \ldots, n+m-1$$, so that the characteristic polynomial in the complex variable s,

$$p_d(s) = s^{n+m} + \lambda_{n+m-1}s^{n+m-1} + \ldots + \lambda_1 s + \lambda_0$$

(7)

exhibits all its roots sufficiently far from the imaginary axis, in the left half of the complex plane, then the trajectories for $$e_y$$ and for its time derivatives globally asymptotically converge, in an exponentially dominated manner, towards a small as-desired vicinity of...
the origin of the estimation error phase space, \( \{e_y, \dot{e}_y, \ldots, e_y^{(n-m-1)}\} \), where they remain ultimately bounded. The further away the roots are located in the left half of the complex plane, the smaller the vicinity of ultimate boundedness around the origin of the estimation error phase space. To prove this result, we proceed as follows: let \( x = (e_1, \ldots, e_{n+m})^T \) denote the phase variables of (6). The perturbed linear system (6) is of the form: \( \dot{x} = A x + b \phi^{(m)}(t) \), with \( A \) being a Hurwitz matrix written in companion form and \( b \) is a vector of zeroes except for the last component being equal to 1. Let \( Q \) be a symmetric positive definite matrix. Then, from Lyapunov stability theory, it follows that, thanks to \( A \) being a Hurwitz matrix, there exists a positive definite symmetric matrix, \( P \), such that \( A^T P + PA = -Q \). The Lyapunov function candidate, \( V(x) = \frac{1}{2} x^T P x \), evaluated along the solutions of the system \( \dot{x} = A x + b \phi^{(m)}(t) \), exhibits a strictly negative time derivative everywhere outside the sphere: \( S = \{ x \in R^{n+m+1} \mid \| x \| \leq K \sqrt{\sigma_{\text{max}}(Q)} \} \). Hence, all trajectories starting outside this sphere converge towards its interior, and all those trajectories starting inside this sphere will never abandon it. The more negative the real part of the dominant eigenvalues of \( A \), the larger the value of \( [\sigma_{\text{max}}(Q)] \) and, hence, the smaller the radius of the ultimate bounding sphere in the \( x \) space.

From (5) it follows that

\[
    z_1 = \phi(t, y_1(t), y_2(t), \ldots, y_n(t)) - \lambda_m e_1 - \dot{e}_n
\]  

Hence, as \( e_1 \) and \( e_n \) evolve towards the small bounding sphere in the estimation error phase space, the trajectory of \( z_1 \) tracks arbitrarily close the unknown function, \( \phi(t, y_1(t), y_2(t), \ldots, y_n(t)) \). Clearly, \( z_1 \) converges towards a vicinity of \( \phi^{(i-1)}(t) \), \( i = 1, \ldots, m \). From the definition of the estimation errors for \( y \) and its time derivatives, it follows that \( \dot{\tilde{y}}_j, j = 1, \ldots, n \) reconstruct, in an arbitrarily close fashion, the time derivatives of \( y \).

Let \( u \) be a scalar input and let \( \psi(t, y, u) \) be a perfectly known smooth scalar function with, \( \partial \psi / \partial u \), uniformly bounded away from zero for all \( y \); so that \( \psi(t, y, \theta(t, y, v)) = v \) with \( u = \theta(t, y, v) \) whenever \( \psi(t, y, u) = u \). The above result extends immediately to nonlinear flat systems, with flat output \( y \), of the form: \( y^{(n)} = \phi(t, y, \dot{y}, \ldots, y_1, y) \), by considering the observer:

\[
    \dot{\hat{y}}_j = \hat{y}_{j+1} + \lambda_{j+m-1} (y_1 - \hat{y}_1), \quad j = 1, 2, \ldots, n - 1
\]

\[
    \dot{\hat{y}}_n = \psi(t, y, u) + z_1 + \lambda_m (y_1 - \hat{y}_1)
\]

\[
    \dot{z}_i = z_{i+1} + \lambda_{m-j} (y_1 - \hat{y}_1), \quad i = 1, 2, \ldots, m - 1
\]

\[
    \dot{z}_m = \lambda_0 (y_1 - \hat{y}_1)
\]

Given a smooth output reference trajectory, \( y^*(t) \), a GPI observer-based controller, including an active disturbance rejection term \( z_1 \), is readily given by

\[
    u = \theta(t, y_1, v),
\]

\[
    v = -z_1 + [y^*(t)]^{\alpha} - \sum_{i=0}^{n-2} \kappa_i (\hat{y}_{i+1} - [y^*(t)]^{\alpha})
\]  

(10)

where the set of parameters \( \kappa_i, i = 0, \ldots, n - 2 \) is specified so that the associated polynomial, \( p_i(s) \), in the complex variables \( s \),

\[
    p_i(s) = s^n + \kappa_{n-1} s^{n-1} + \cdots + \kappa_1 s + \kappa_0
\]  

(11)

is a Hurwitz polynomial with all roots located sufficiently far from the imaginary axis in the complex plane.

The closed-loop tracking error system, with \( e = y - y^*(t) \), evolves according to the \( n \)-th order perturbed linearly dominated dynamics

\[
    e^{(n)} + \sum_{i=0}^{n-1} \kappa_i e^{(i)} = \phi(t, y_1(t), y_2(t), \ldots, y_n(t)) - z_1
\]

\[
    + \sum_{i=0}^{n-2} \kappa_i e^{i+1}
\]  

(12)

where we have used, as before, the observer estimation error vector components: \( e_1 = e_1 = y_1 - \hat{y}_1 = y - \hat{y}_1 \), \( e_2 = y_2 - \hat{y}_2 \), etc. Given the ultimate asymptotic convergence of \( z_1 \) to an arbitrarily small neighbourhood of \( \phi(t, y_1(t), y_2(t), \ldots, y_n(t)) \) and the convergence of the observer estimation errors \( e_j, j = 1, \ldots, n \) to a small vicinity of the origin of the estimation error phase space, the linear dynamics in (12) is perturbed by a right-hand side whose terms are ultimately uniformly absolutely bounded signals confined to a sufficiently small neighbourhood of the origin. The previous Lyapunov stability result similarly applies and the tracking error, \( e \), converges to a small as desired vicinity of zero. The general assumptions and the use of a high-gain observer followed by the active disturbance cancelation lead to a form of the separation principle already explored in Atassi and Khalil (2001).

As a final remark, it should be pointed out that low-pass filtering is required for the implementation of the GPI observer-based algorithm, along with appropriate ‘clutching’ of the observer output signals (see Sira-Ramirez et al. 2010, 2009a) for details).

Real life noises do not entirely preclude the application of high-gain observers, as it can be inferred from the experimental results here presented.

3. Linear control of Chua’s circuit

Consider the modified version of Chua’s circuit depicted in Figure 1, including an external current
source of value $u$, acting as a control input variable to the circuit. The mathematical model of the circuit is given by,

$$
\begin{align*}
C_1 \dot{x}_1 &= \frac{1}{R} (x_2 - x_1) - \varphi(x_1) + u \\
C_2 \dot{x}_2 &= \frac{1}{R} (x_1 - x_2) - x_3 \\
L \dot{x}_3 &= x_2, \quad y = x_3
\end{align*}
$$

with the nonlinear function $\varphi(x_1)$ given by

$$
\varphi(x_1) = m_0 x_1 + \frac{(m_1 - m_0)}{2} (|x_1 + B_p| - |x_1 - B_p|)
$$

where $x_1, x_2$ represent the voltages on the capacitors $C_1, C_2$. The variable $x_3$ represents the current through the inductor $L$, while $\varphi(x_1)$ is the current through the nonlinear resistor (known as Chua’s diode), $m_0, m_1, B_p$ are fixed, but possibly unknown, constants.

Notice that the controlled system is flat (Fliess et al. 1995), with $x_3$ being the flat output or the linearising output. Indeed, all the system variables including the control input $u$, may be expressed in terms of $y = x_3$ and a finite number of its time derivatives:

$$
\begin{align*}
x_1 &= R L C_2 \dot{y} + L \dot{y} + R y \\
x_2 &= L \dot{y} \\
x_3 &= y
\end{align*}
$$

and

$$
\begin{align*}
u &= R L C_1 C_2 y^{(3)} + L (C_1 + C_2) \dot{y} + R C_1 \dot{y} + y \\
&\quad + m_0 (R L C_2 \dot{y} + L \dot{y} + R y) + \frac{(m_1 - m_0)}{2} \times \\
&\quad \left( |R L C_2 \dot{y} + L \dot{y} + R y + B_p| - |R L C_2 \dot{y} + L \dot{y} + R y - B_p| \right)
\end{align*}
$$

Under this complete differential parametrisation, and for the purposes of constructing a GPI observer-based controller, the resulting input-to-flat output dynamics, which is also free of any zero dynamics, can be obtained from (15) as the following simplified system:

$$
y^{(3)} = \frac{1}{R L C_1 C_2} u + \xi(t)
$$

where $\xi(t)$ lumps the nonlinear state-dependent terms in (15) which contains the uncertain parameters of the Chua’s diode. Due to the uniformly absolutely bounded responses of the circuit, the input signal $\xi(t)$ may be considered as an unknown, but uniformly absolutely bounded, input. As seen above, this signal can be on-line approximately estimated by means of a GPI observer. Such an on-line estimation allows the subsequent cancelling of $\xi(t)$ from the input-to-flat output dynamics, through the appropriately devised, GPI observer-based, active disturbance rejection control law. The nonlinear output trajectory tracking controller design task is, thus, reduced to that of a linear output feedback controller on a third order chain of integrators.

### 3.1 Problem formulation

Given as a smooth output reference signal $y^*(t)$, the output $z(t)$ of the following perfectly known Lorenz system,

$$
\begin{align*}
\dot{z}_1 &= \sigma (z_2 - z_1) \\
\dot{z}_2 &= r z_1 - z_2 - z_1 z_3 \\
\dot{z}_3 &= z_1 z_2 - b z_3 \\
z(t) &= \varepsilon z_1(t)
\end{align*}
$$

it is desired to force the Chua’s circuit output $y = x_3$ to accurately track the given trajectory $y^*(t) = z(t)$, independently of the possible unmodelled external disturbance inputs and regardless of the endogenous disturbance input $\xi(t)$, affecting the input-to-flat output simplified dynamics (16).

### 3.2 A GPI observer-based disturbance rejection control for Chua’s circuit

Figure 2 depicts a block diagram of the proposed observer-based control. The GPI observer processes the input and the output signals of the system to produce an estimate the lumped signal $\xi(t)$, and of the states $\dot{y}, \ddot{y}$. As a result, the estimate of $\xi(t)$ may be used in combination with a linear output feedback
controller to perform, thanks to disturbance cancelation, the tracking of the Lorenz reference signal $z(t)$.

We propose the following GPI observer-based control, using a lumped disturbance internal model requiring four iterated output error integral injections for its approximate cancelation, i.e. $m = 5$

$$u = RLC_1 C_2 \left[ \left( y(t)^3 \right) - \kappa_2 (y - y^*) \right]$$

$$- \kappa_0 (y - y^*) - \tilde{\xi}(t)$$

$$\begin{align*}
\dot{y}_1 &= y_2 + \lambda_7 (y - y_1) \\
\dot{y}_2 &= y_3 + \lambda_6 (y - y_1) \\
\dot{y}_3 &= \frac{1}{RLC_1 C_2} u + z_1 + \lambda_5 (y - y_1) \\
\dot{z}_1 &= z_2 + \lambda_4 (y - y_1) \\
\dot{z}_2 &= z_3 + \lambda_3 (y - y_1) \\
\dot{z}_3 &= z_4 + \lambda_2 (y - y_1) \\
\dot{z}_4 &= z_5 + \lambda_1 (y - y_1) \\
\dot{z}_5 &= \lambda_0 (y - y_1) \\
\dot{\xi}(t) &= z_1 \\
\dot{y}(t) &= y_1, \quad \dot{\hat{y}}(t) = y_2 \quad \dot{\hat{y}}(t) = y_3
\end{align*}$$

where the characteristic polynomial associated with the estimation error is given by

$$p_{ob}(s) = s^8 + \lambda_7 s^7 + \lambda_6 s^6 + \cdots + \lambda_1 s + \lambda_0$$

and the characteristic polynomial of the predominantly linear closed-loop tracking error is

$$p_c(s) = s^3 + \kappa_5 s^2 + \kappa_1 s + \kappa_0$$

By choosing, $\lambda_0, \ldots, \lambda_7$, such that $p_{ob}(s)$ exhibits the form, $(s^2 + 2\xi_1 \omega_{no1} s + \omega_{no1}^2)^2 (s^2 + 2\xi_2 \omega_{no2} s + \omega_{no2}^2)^2$, with $\xi_1$, $\xi_2$, $\omega_{no1}$, $\omega_{no2}$ strictly positive constants, the reconstruction error $e = y - y_1$ is ultimately confined to a small as desired vicinity of the origin of the reconstruction error phase space, provided the roots of $p_{ob}(s)$ are located sufficiently to the left of the imaginary axis in the complex plane. Analogously, selecting $\kappa_0, \kappa_1, \kappa_2$, based on the desired form of the dominant characteristic polynomial, $(s^2 + 2\xi \omega_c s + \omega_c^2)^2 (s + p_c)$, with $\xi, \omega_c, p_c > 0$, we ensure the tracking error to exponentially converge towards a small region around the origin of the tracking error phase space. This vicinity becomes smaller by increasing, in absolute value, the real part of the roots of $p_c(s)$ in the left half of the complex plane.

4. Experimental results

The previously described linear output feedback control law was devised for an actual Chua’s circuit prototype, constructed on the basis of the work of Torres and Aguirre (2000) which handles low-frequency chaotic oscillations, thus avoiding time reparameterisations in the model synthesis.

Figure 3 shows the Chua’s diode realisation, based on operational amplifiers (Kennedy 1992), and Figure 4 shows the schematic diagram of the inductor equivalent circuit. The following set of circuit parameters was used: $C_1 = 23.5 \mu F$, $C_2 = 235 \mu F$, $R = 1550 \Omega$. The equivalent inductance of the realisation was, $L = L_{eq} = 42.3$ H. The nonlinear parameters of Chua’s diode were set to be: $m_0 = -0.409$ ms, $m_1 = -0.758$ ms, $B_p = 1.8$ V. The passive components for the op-amp realisation were chosen as: $R_1 = R_2 = 220 \Omega$, $R_3 = 22 k\Omega$, $R_4 = 22 k\Omega$, $R_6 = 3.3 k\Omega$, $R_7 = R_8 = R_9 = 1 k\Omega$, $R_{10} = 1.8 k\Omega$ and $C_1 = 23.5 \mu F$. All operational amplifiers were integrated circuits of the LF412 type. The GPI control was implemented by means of a National Instruments Data Acquisition Card PCI-6259. The control output was synthesised through the analogue output, and the control law was devised using Matlab Simulink software in a real time implementation environment using the xPc target hardware in the loop simulation with a sampling period of 0.1 ms. Figure 5 depicts the experimental implementation of the modified Chua’s circuit.

Concerning the GPI observer-based control, the design parameters of the characteristic polynomial of the observer were set to be: $\xi_1 = 2$, $\omega_{no1} = 50$, $\xi_2 = 2$, $\omega_{no2} = 70$. The characteristic polynomial of the closed-loop control was chosen to be of the form $(s^2 + 2\xi \omega_c s + \omega_c^2)(s + p_c)$, with $\xi_c = 1$, $\omega_c = 50$, and $p_c = 50$.

We tested the performance of the GPI observer-based feedback control in the challenging task of having the controlled Chua’s circuit flat output, $y$, track a particular output, $z(t)$, of an uncontrolled

![Figure 3. Operational Amplifier realisation of Chua’s diode.](image-url)
Lorenz chaotic system, with \( \sigma = 10, r = 28, b = \frac{8}{3} \) and \( \epsilon = 0.75 \times 10^{-4} \).

We let \( z = y^*(t) \) become the reference signal for the flat output \( y \) of the controlled Chua’s circuit and used the observer-based GPI control synthesis for the corresponding output reference trajectory tracking problem. We let Chua’s circuit evolve without any control action for a period of 30 s, and then we switched on the GPI observer-based controller. Figure 6 depicts the performance of the controller in the tracking task and it is evident how the tracking error signal, \( y - y^*(t) \) (both expressed in Amperes [A]), remains in a small region around the origin of the error space. On the other hand, Figure 7 shows the behaviour of the \( x_1, x_2 \) state variables of the Chua’s circuit (both expressed in Volts [V]). Figure 8 illustrates the results of the disturbance estimation and the acting feedback control input signal. Figure 9 shows the implementation results using an oscilloscope.

### 4.1 Robustness with respect to the control gain parameter

Finally, to test the robustness of the controller with respect to the lack of precise knowledge in the gain parameter \( a = 1/RLC_1C_2 \), we hypothesise an uncertainty percentage factor, \( f \), of the actual value of the parameter \( a \). The parameter \( f \) depicts an exact knowledge of the gain parameter \( a \) whenever \( f = 1 \). The gain parameter to be used, both, in the proposed controller and the proposed GPI observer, for robustness evaluation through computer simulations, is taken to be of the form: \( \hat{a} = (1/RLC_1C_2)f \). One proceeds to obtain performance graphs for various values of \( f \) taken around the nominally ideal value of 1. These performance evaluation graphs may be made in terms of an integral square error criterion on the trajectory tracking accuracy. Consider the following performance index:

\[
ISE_f(t) = n \int_0^t [y(t) - y^*(t)]^2 dt
\]
with $n_f$ being a normalisation factor that sets the steady state value of the index ($ISE_f(\infty)$) to 1, when $a$ is perfectly known and $f$ is taken to be 1. Figures 10 and 11 depict the time evolution of the performance index $ISE_f(t)$ for different values of $f$. It is found that for $f$, extracted from the interval set: $[0.3, 2.5]$, the performance index stabilises to a constant value. For values outside this interval, the performance index trajectory grows without limit indicating a failure of the tracking method.

5. Concluding remarks

In this article, we have proposed a linear active disturbance rejection feedback control approach for the output trajectory tracking task in a controlled version of Chua’s circuit with uncertain parameters. The proposed linear controller design methodology is based on the facts that (1) the nonlinear uncontrolled system is easily made to be flat, thanks to the possibilities of choosing a physically meaningful control input channel and (2) one can simplify, for observer design purposes, the highly nonlinear input-to-flat output representation of the circuit to that of a linear perturbed chain of integrations, in which only the order of integration of the system and the control input gain need to be known. We have shown, in an actual laboratory implementation, that the proposed linear output feedback control method efficiently results in a rather accurate closed-loop trajectory tracking. This was particularly valid in an output
trajectory tracking, on the part of the Chua’s circuit, of a chaotic system’s output generated by an unrelated Lorenz system.

The proposed linear GPI observer-based control design methodology can be extended to the linear feedback control of some other controlled versions of chaotic, and even hyper-chaotic, systems. The relative freedom of choosing the control input channel results in a controlled system which is, generally speaking, ‘easy’ to control when the flatness property is either induced, or invoked on a certain measurable output of the circuit. The use of the proposed controller design method is specially suitable in forced chaotic synchronisation tasks, specially when a controlled chaotic system output is made to behave as that of a given different uncontrolled chaotic system. This particular possibility may prove to be useful in ‘controlled chaotic encryption’ tasks.

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Note
1. This assumption cannot be verified a priori when φ(·) is completely unknown. However, in cases where the nonlinearity is known except for some of its parameters, as it is the case of the Chua’s system, its validity can be assessed with some work.

References


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